

# ADSL Line Driver/Receiver Design Guide, Part 1

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## Introduction

Consumer desire for faster Internet access is driving the demand for very high data rate modems. A digital subscriber line (DSL) implementation speeds data to and from remote servers with data rates of 512Kbps to 8Mbps, much faster than current 56Kbps modem alternatives. This speed of data communication is providing the Internet with the capability to transfer information in new formats such as full-motion video, while

greatly improving the timeliness of conventional information access.

One very important feature of DSL technology is that the connection is handled through a normal telephone line; therefore, no special high speed cables or fiber optic links are required and every home and office is most likely DSL ready. Another feature is that the data interface can operate simultaneously with normal voice communication over the same tele-

phone line. This allows the modem to be connected at all times and not interfere with the use of the same line for normal incoming and outgoing phone calls or faxes.

The real “magic” of DSL technology stems from the application of digital signal processing (DSP) algorithms and data coding schemes. The implementations have built-in intelligence to accommodate the wide variations of data transmission signal conditions

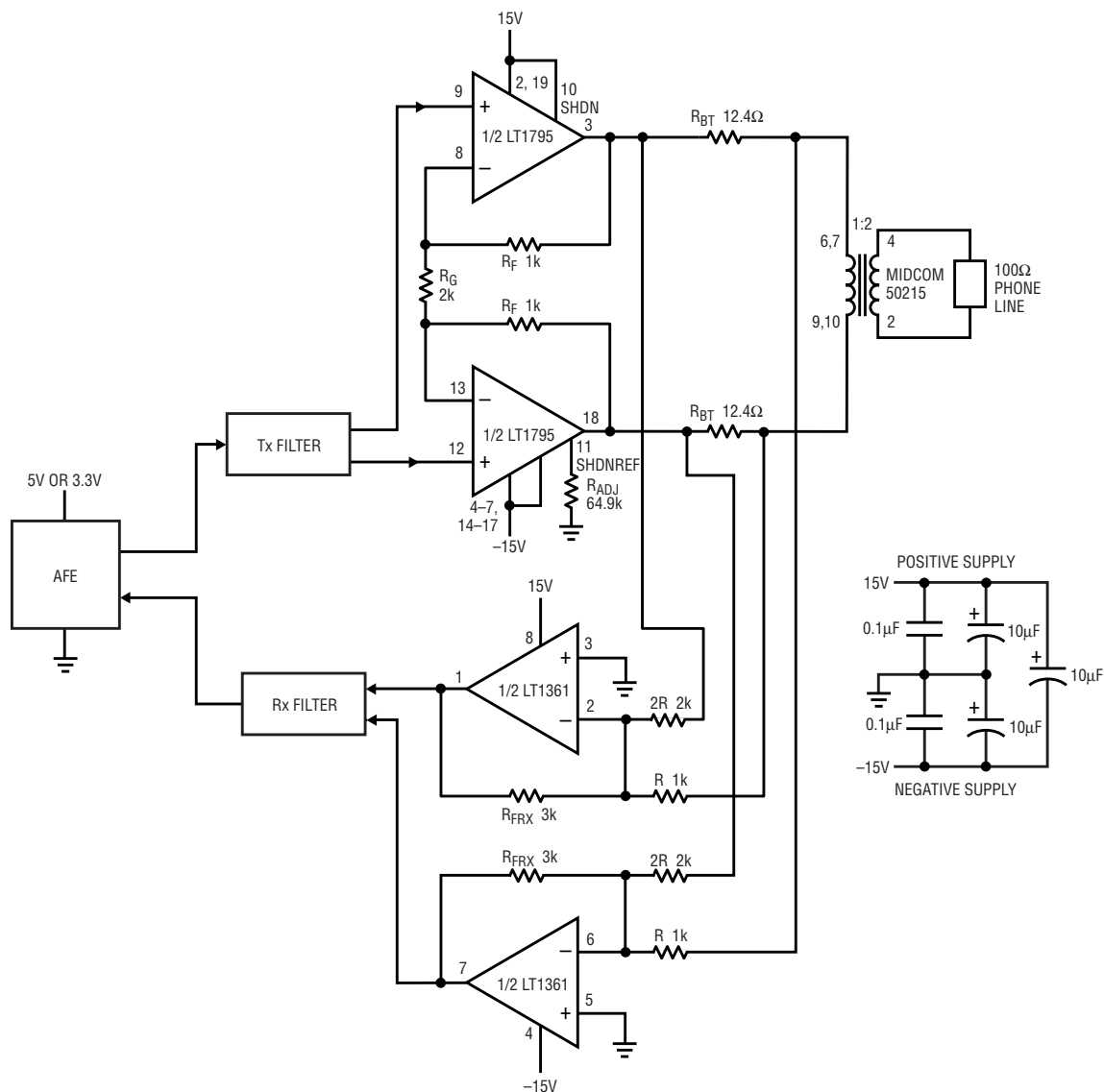
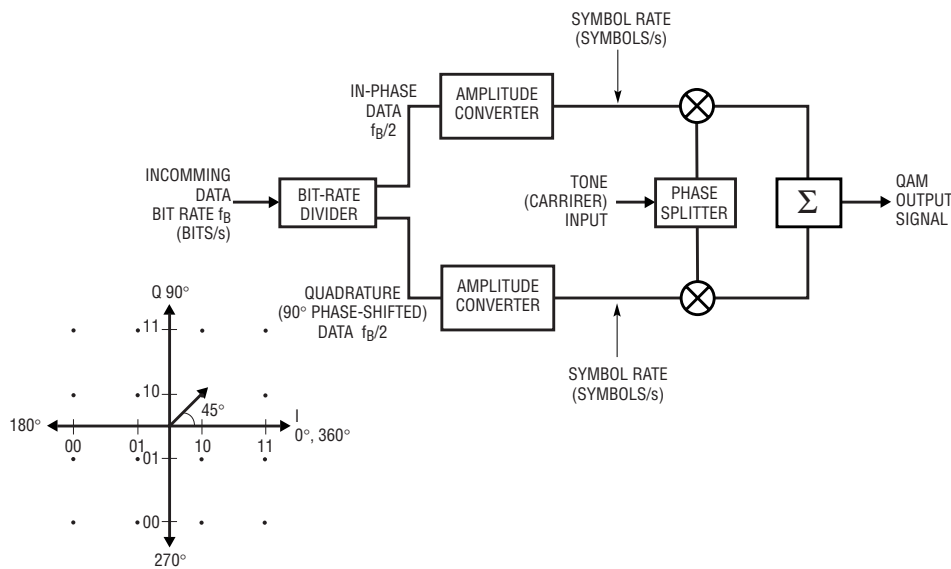


Figure 1. Central-office ADSL transceiver



CODE		LEVELS		VECTOR	
I	Q	I (2MSB)	Q (2LSB)	MAG	ANGLE (°)
00	00	-3	-3	4.2	225
00	01	-3	-1	3.2	198
00	10	-3	1	3.2	162
00	11	-3	3	4.2	135
01	00	-1	-3	3.2	252
01	01	-1	-1	1.4	225
01	10	-1	1	1.4	135
01	11	-1	3	3.2	108
10	00	1	-3	3.2	288
10	01	1	-1	1.4	315
10	10	1	1	1.4	45
10	11	1	3	3.2	72
11	00	3	-3	4.2	315
11	01	3	-1	3.2	342
11	10	3	1	3.2	18
11	11	3	3	4.2	45

Figure 2. Quadrature amplitude modulation

encountered with each connection through the telephone switching network. Sophisticated ASICs have been developed to provide small modems for PCs and handheld devices and the ability to compact many DSL lines on a single PCB card for telephone central-office deployment.

However, as is the case with almost any system, DSL still requires fundamental operational amplifier functions to put the signal on to the phone line and to pick off the small signals received at the other end. Although many system designers are competent and comfortable with DSP and all things digital, they often find their understanding of analog issues to be a bit rusty when it comes to implementing the physical connection to and from the telephone line. This series of articles will provide an overview of the requirements placed on the amplifiers and provide guidelines to component selection and the implications on distortion performance and power consumption and dissipation, the most important system issues related to the analog components.

Figure 1 shows a complete central office DSL line driver/receiver. This is the basic circuit topology that provides differential transmit signal drive to the line and detection of the differential received signal. The full requirements of DSL are easily met by using devices from Linear Tech-

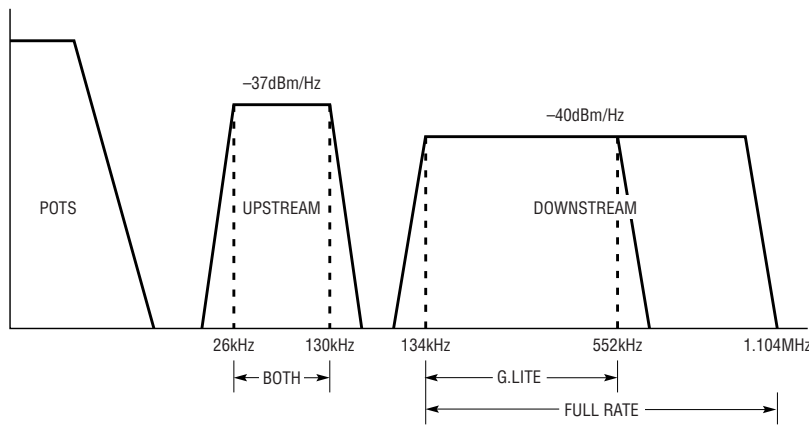
nology's broad line of high speed power amplifiers for the driver and high speed, low noise dual amplifiers for the receiver. Using either current feedback or voltage feedback topologies, the family of drivers consists of amplifiers with bandwidths from 35MHz to 75MHz, slew rates in excess of 200V/ $\mu$ s with output current capability from 125mA to over 1 amp. The receiver family combines similar high speed performance with low noise, less than 10nV/ $\sqrt{\text{Hz}}$ , and low quiescent operating current, less than 10mA. The devices shown in Figure 1 are the LT1795 500mA output current, 50MHz bandwidth dual op amp and the LT1361 50MHz dual amplifier with input noise voltage of 9nV/ $\sqrt{\text{Hz}}$  and total supply current of only 10mA.

Although there are several variations of DSL technology (SDSL, HDSL, HDSL2, VDSL and ADSL, to name a few) the requirements placed on the amplifiers for these different standards are very similar. The major difference between the approaches, as they affect the line driver, is the amount of power actually put on to the phone line by the line-driver amplifier. For simplicity, these articles will focus on the most recently approved standard, ADSL (asymmetric DSL), but the concepts discussed apply equally to any of the other standards.

This first installment will provide an overview of the requirements of ADSL and how it is done, as well as a discussion of the circuit topology and the requirements for the components used for implementation.

### The Requirements for ADSL

The full specifications for ADSL are contained in two ITU (International Telecommunications Union) documents called G.992.1, for systems often referred to as Full-Rate ADSL or G.dmt, and G.992.2, a lower data rate approach often called G.Lite. Both systems use a technique called discrete multitone, or DMT, for transmitting data. With DMT, a frequency band up to 1.2MHz is split up into 256 separate tones (also call sub-carriers) each spaced 4.3125kHz apart. With each tone carrying separate data, the technique operates as if 256 separate modems were running in parallel. To further increase the data transmission rate, each individual tone is quadrature amplitude modulated (QAM). As shown in Figure 2, the data to be transmitted is used to create a unique amplitude and phase-shift characteristic for each carrier tone, through the combination of I and Q data, called a symbol. The symbols represented by each tone are updated at a 4kHz rate or 4000 symbols per second. Full Rate ADSL uses up to 15 bits of data to create



**Figure 3. DMT channel allocation**

route to and from the central office. The total power required can be determined from the following equation:

$$\text{LINE POWER (dBm)} = \text{PSD (dBm/Hz)} + 10 \cdot \text{Log}(F_{\text{MAX}} - F_{\text{MIN}})$$

The downstream power requirements are much higher than the upstream requirements because of the wider bandwidth used for the transmission. For this reason, Full Rate ADSL requires more line power than G.Lite for downstream transmissions. Upstream power is the same for both Full Rate and G.Lite

each symbol. This results in a theoretical maximum of 60Kb/s for each tone. If all 256 tones are used in parallel, the total theoretical data rate can be as fast as 15.36Mb/s. For G.Lite, only 8 bits are used per symbol with only half of the carrier tones used for a theoretical maximum data rate of 4.096Mb/s.

In an actual DSL application, the tones are allocated for use depending on the direction of communication, as shown in Figure 3. Most of the tones are used for communication from the central office (CO) to an end user's PC modem (often referred to as the CPE or customer premises equipment). This direction of communication is called "downstream." The direction of communication from a PC modem to the central office (and, ultimately, to an Internet server) is called "upstream." The use of more tones for the downstream direction makes sense from an Internet-access point of view, because most users download more information than they upload. Most upstream communication with a server is simply to request information to be sent quickly downstream. This difference in data rates up- and downstream is the reason ADSL is called asymmetric DSL.

Also indicated in Figure 3 is the power spectral density (PSD) of all of the tones used. This determines the amount of signal power that needs to be put on to the phone line. The power levels are restricted to minimize cross-talk and interference into other phone lines contained in wire bundles en

**Table 1. ADSL requirements**

Parameter		Full Rate ADSL Downstream	ADSL G.Lite Downstream	Full Rate ADSL or G.Lite Upstream
Characteristics	Channels Used	31 to 256	31 to 128	6 to 30
	Frequency Band (kHz)	133.7 to 1104	133.7 to 552	25.8 to 129.4
	Bandwidth (kHz)	970.3	418.3	103.5
	Power Spectral Density, PSD (dBm/Hz)	-40	-40	-37
	Line Power (dBm)	20	16.3	13
Electrical Requirements	RMS Line Power (mW)	100	43	20
	Line Impedance ( $\Omega$ )	100	100	100
	RMS Line Voltage (V)	3.1	2	1.4
	RMS Line Current (mA)	31	21	15
	Peak-to-Average Ratio, PAR	5.3	5.3	5.3
	Peak Line Voltage (V)	16.5	11	7.6
	Peak-to-Peak Line Voltage (V)	33	22	15.2
	Peak Line Current (mA)	170	110	76
	Peak Line Power (mW)	2725	1175	580
Theoretical Data Rates	Bits/Symbol	15	8	15 (Full) 8 (G.Lite)
	Bits/Channel (KBits/s)	60	32	60 (Full) 32 (G.Lite)
	Max Data Rate for Channels Used	13.5Mb/s	3.1Mb/s	1.4Mb/s (Full) 768Kb/s (G.Lite)

implementations. As will be seen, the line power requirement is the most significant factor in designing a line driver for a particular application.

Table 1 is a summary of the characteristics, electrical requirements and maximum data rates for ADSL modems.

The following are important items to note:

The phone line characteristic impedance for ADSL is 100Ω. This is used to determine the voltage and current required to provide the proper line-power level.

The term PAR stands for peak-to-average ratio. This term is similar to the more common term of crest factor. This determines the peak value of the voltage put on the line over time with respect to the RMS voltage level:

$$V_{\text{PEAK}} = \text{PAR} \cdot V_{\text{RMS}}$$

The DMT signal placed on the line looks basically like white noise, because many different frequencies of rapidly changing amplitude and phase are combined simultaneously. The changes of each tone are considered random as they result from an arbitrary sequence of data bits comprising the transmitted information. Over time, the signals can align and stack up to create a large peak signal. If this large peak is not processed cleanly (for example, if the line-driver amplifier clips) data errors can occur, which must be detected and resent. Transmission errors, particularly over a noisy environment such as phone lines, are inevitable. These errors are identified by a term called the bit-error rate (BER); an acceptable level to maintain fast and accurate data transmission is one error per every  $10^7$  symbols. The PAR is determined by the probability of the random line signal reaching a certain peak voltage during the time interval required for  $10^7$  symbols. For the DMT signal, this peak value is 5.3 times the RMS signal level. This factor is very important in determining both the minimum supply voltage required to prevent clipping of the signal and also the peak output current capability of the line driver.

Although the data rates shown in Table 1 are impressively fast, they are, indeed, theoretical. In an actual connection over the phone line, all manner of interference sources will alter the frequency response over the 1.2MHz band. These interference sources can contaminate or attenuate many of the carrier tones to render them completely unusable, or useful but with less than the maximum possible number of data bits encoded. Additionally, higher frequency tones are attenuated more than the lower ones, particularly over longer lengths of phone line used to make the connection.

Another issue that can render particular tones unusable or create transmission errors is distortion from the amplifier driving the line. Distortion products, whether harmonic, intermodulation or from signal clipping, from any of the carrier tones, create signal energy in the frequency spaces used by other tones. This energy also contaminates the data content of the tones and can result in fewer tones being used for data transmission. If many tones are unusable or their data handling capability is reduced, the actual data rate for any given connection can be significantly less than the theoretical maximum.

One of the best features of a DSL modem is the intelligence built in to obtain the fastest data rate for any set of line conditions. When a connection between a modem and the telephone central office is initiated, the first action to occur is called "training-up." During this interval, both ends transmit maximum power in each channel in an effort to determine

which channels are best suited for use. The DSP algorithms will automatically pack the most data into the best transmission channels to maximize the data rate for a particular connection. Figure 4 illustrates a typical line spectrum during a training-up interval in a G.Lite example, as measured at the central office end.

## A Typical ADSL Line Driver/Receiver Circuit

Referring to Figure 1, the components shown will implement a Full Rate ADSL central office (downstream) port. A discussion of the circuit topology and aspects important for component selection follow.

## Transformer Coupling

A transformer is used to connect the transceiver to the phone line, mainly to provide isolation from the line. The turns ratio of the transformer can be used to provide gain to the transmitted signal. This turns ratio has a major effect on the power supply voltages for the line-driver amplifiers. By stepping up the signal from the driver to the line via the transformer, the amount of voltage swing needed by the amplifiers is reduced. As an ideal transformer has equal power in the primary and secondary, while the voltage is stepped up, the current is stepped down. The consequences of using a step-up transformer are beneficial in that lower, more conventional supply voltages can be used, but the amplifiers must have higher current driving capability.

The limit on the turns ratio is primarily a function of the sensitivity of the receive circuitry. Step-up transformers will, unfortunately, step-down the signal received from the phone line. Further attenuation of the received signal by the transformer in addition to the inherent transmission line attenuation can cause the receiver to stop functioning. If this occurs, the modem will disconnect from the line.

A transformer should be selected for a flat, distortion-free frequency response from 20kHz to 2MHz to cover the full frequency spectrum for an

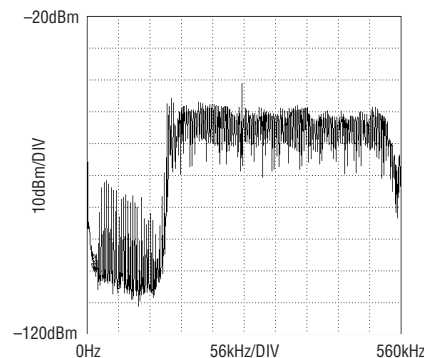
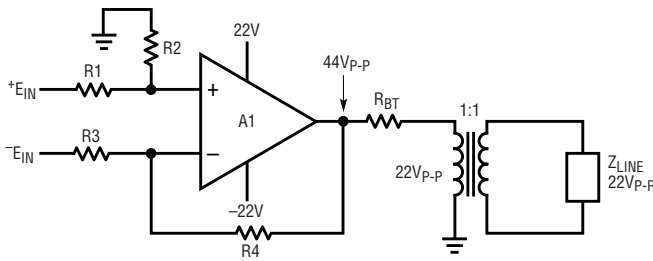


Figure 4. G.Lite training-up spectrum



**Figure 5a. A single-ended driver requires a high supply voltage to produce the desired peak-to-peak swing of the DMT signal on the phone line.**

ADSL transmission. Minimal insertion loss in the transformer over the same frequency range is also desirable. Insertion loss, usually specified in dBm, is power lost in the transformer. The driver amplifier must provide this additional power in order to maintain the required signal power level on the phone line.

**Transformer Termination Resistors**

The two resistors (called back-termination resistors) shown between the amplifier outputs and the primary of the transformer are inserted for two reasons: to provide a means for detecting the received signal and to make the impedance of the modem match the impedance of the phone line. The receiver circuit is two difference amplifiers that provide gain to the small signals that appear across the termination resistors. The connection and scaling of the input resistors to the receiver amplifiers are purposely set to provide a first-order cancellation of the simultaneously occurring transmit signal. This technique is called “echo cancellation” and the circuit topology is called a “2-wire to 4-wire hybrid” (the 2-wire phone line interfaces with four wires, the two differential driver lines and the two receive signal lines). The cancellation of the transmitted signal from the received signal path is not perfect. Due to signal phase shifts and resistor mismatching, a factor of 6dB to 20dB of attenuation is typical, with higher frequencies being cancelled less. The amount of transmitted signal that remains is cancelled digitally by DSP echo-canceling algorithms.

The value of the termination resistors is a function of the line impedance

and the transformer turns ratio. The turns ratio,  $n$ , is defined by the number of turns of the winding connected to the phone line (the secondary) divided by the number of turns of the driver side winding (the primary). To make the modem impedance match the line impedance, the total impedance across the primary winding is determined by the following relationship:

$$R_{PRIMARY} = \frac{Z_{LINE}}{n^2}$$

To provide balanced drive to the primary of the transformer, so that each power amplifier shares the work load evenly, each termination resistor is set to a value of one-half of  $R_{PRIMARY}$ .

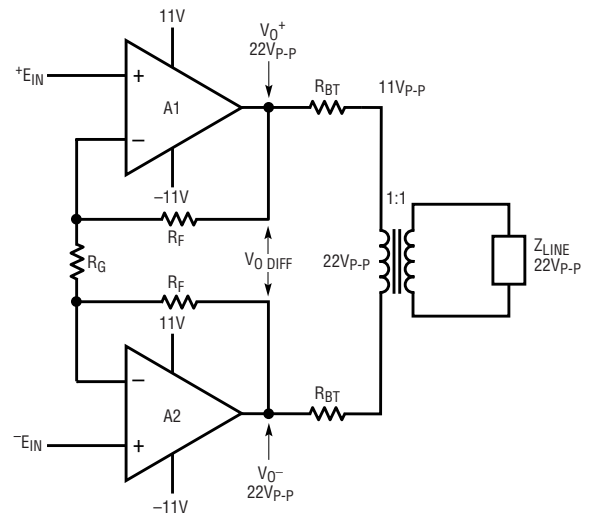
This value of termination resistance on the primary is also optimal for receiving maximum power from the line. The received signal on the phone line,  $e_{RX}$ , driving the secondary through the line impedance,  $Z_{LINE}$  (nominally 100Ω) will develop signal power in the primary per the following relationship:

$$RECEIVED\ PRIMARY\ POWER = \frac{e_{RX}^2}{\frac{Z_{LINE}^2}{n^2 \cdot R_{PRIMARY}} + 2 \cdot Z_{LINE} + n^2 \cdot R_{PRIMARY}}$$

which is also at a maximum when

$$R_{PRIMARY} = \frac{Z_{LINE}}{n^2}$$

While the termination resistors serve an important purpose, they also create significant signal and power loss. With the resistors set to their



**Figure 5b. A differential driver achieves the same swing with half the supply voltage of the single-ended driver.**

proper value, one-half of the power delivered by the amplifiers is dissipated in these resistors. To deliver 100mW of signal power to the phone line, for example, requires the driver amplifiers to output at least 200mW of power.

**Why Differential Drive?**

Two amplifiers configured as a differential gain stage are typically used to provide signal drive to the primary of the transformer. There are two reasons for this configuration: it reduces the supply voltage to the amplifiers by a factor of two and also cancels any even harmonic distortion nonlinearity contributed by the amplifiers.

With single-ended drive of the primary, the supply voltage for the amplifier must be large enough to provide the full peak-to-peak signal swing of the DMT signal placed on to the phone line. With differential drive, each amplifier contributes just one-half of the peak signal amplitude; therefore, the total supply voltage is only one half the peak-to-peak voltage level placed on the line. This is shown conceptually in Figure 5. This reduction in supply voltage allows the use of the standard power supply voltages available in computers for the high speed DSL modem card.

A differential amplifier will ideally cancel all even harmonic distortion products. This is due to the application of a signal that is the difference between two signals, one signal being

an inverted version of the other, to the primary of the transformer. This can be shown mathematically by representing the linear output signals of the amplifiers as a power series:

Each output is a linear function of the input signal:

$$V_0 = f(E_{IN})$$

which, represented as a power series, is

$$V_0 = a_1 E_{IN} + a_2 E_{IN}^2 + a_3 E_{IN}^3 + a_4 E_{IN}^4 + a_5 E_{IN}^5 \dots$$

The inputs to the differential amplifier are  $E_{IN}^+$  and  $E_{IN}^-$ ; therefore:

$$V_0(+) = a_1 E_{IN} + a_2 E_{IN}^2 + a_3 E_{IN}^3 + a_4 E_{IN}^4 + a_5 E_{IN}^5 \dots$$

and

$$V_0(-) = -a_1 E_{IN} + a_2 E_{IN}^2 - a_3 E_{IN}^3 + a_4 E_{IN}^4 - a_5 E_{IN}^5 \dots$$

The differential output of the amplifier stage is

$$V_{ODIFF} = V_0(+) - V_0(-)$$

therefore:

$$V_{ODIFF} = 2a_1 E_{IN} + 2a_3 E_{IN}^3 + 2a_5 E_{IN}^5 + \dots$$

which does not contain any even harmonic products. The complete cancellation of even harmonics depends on the gain and phase-shift matching of the amplifiers and the signal paths over the frequency range of concern.

### Bandwidth, Slew Rate and Noise Requirements of the Amplifiers

High speed amplifiers with bandwidths much wider than the transmitted signal bandwidth should be used to maintain flat gain and constant phase shift of the DMT signals. The amount of gain required in the transmit power amplifiers is dependant on the signal levels provided by the analog front end (AFE), which is a circuit block that provides the interface between the line transceiver and the DSP processor. The gain must be sufficient to put the proper amount of power on the phone line for the DSL standard being implemented (refer to Table 1). The

maximum frequency to be processed by the amplifiers is also a function of the standard being applied; this, in turn, sets the minimum bandwidth required. As a rule of thumb, the gain bandwidth product specification of the amplifiers used should be at least five times the required value to maintain linear accuracy over the transmitted signal spectrum. This specification provides an indication of the distortion-free, high speed signal processing capability of the amplifier. For example, a Full Rate ADSL downstream transmitter with a gain of four and a maximum frequency of 1.1MHz requires a gain-bandwidth of 4.4MHz; therefore, amplifiers should be chosen that have a gain-bandwidth specification of at least 22MHz. Parts with higher bandwidths are even better for preserving excellent gain and phase shift matching over the 1.1MHz band of operation.

The slew rate of the amplifiers used is not so critical, because the signal spectrum is typically band-limited by filter networks. The step response of these filters slows down the rise and fall times of the signals presented to the amplifiers. A slew rate of at least 10V/ $\mu$ s is usually adequate. However, very fast slew rates are essentially free in wideband amplifier designs. Internal biasing currents charging and discharging internal compensation capacitors and individual node capacitances of the circuit determine the slew rate of an amplifier. To produce a high frequency amplifier, circuit-biasing currents are increased to minimize impedances at critical circuit nodes and small geometry transistor structures are used to minimize stray capacitance. This results in very fast slew rates for the amplifier as an inherent byproduct of a high gain-bandwidth product characteristic. Faster slew rates ensure very fast dynamic response and reduced signal distortion.

Low noise characteristics, together with a wide gain bandwidth capability are most important for the amplifiers used in the receive circuitry. On a typical connection, a phone line will have a noise floor

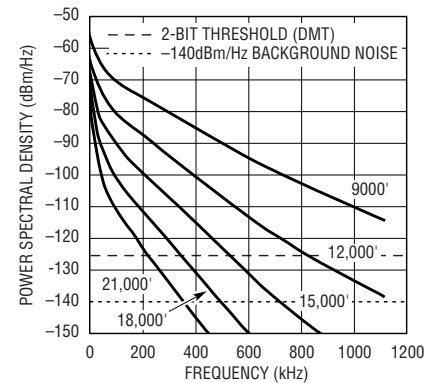


Figure 6. Typical received signal power spectral density, AWG26 loops

power spectral density of -140dBm/Hz. This is equivalent to a noise voltage of 31nV/ $\sqrt$ Hz. The receiver amplifier should have a noise spectral density in the band between 20kHz and 1MHz lower than this level. Linear Technology provides several fast amplifiers with noise voltage spectra of less than 10nV/ $\sqrt$ Hz. Lower noise is required in inverse proportion to the turns ratio of the transformer used to address the attendant reduction in both the noise floor and the received signal.

The amount of signal received is a function of the length of phone line used to make the connection, as shown in Figure 6. This is referred to as the loop length. Very long loop lengths can severely attenuate the transmitted signal, particularly at the higher channel frequencies. The greater the attenuation of a channel, the fewer data bits can be transmitted in that channel, which affects the overall communication data rate. As a rule of thumb, a received signal-to-noise ratio of 18dB allows two data bits to be used in a channel. With each 3dB of additional signal above the noise floor, an extra bit of data can be used. With 45dB to 50dB signal-to-noise ratio, a full 12 bits of data can be exchanged in one channel frequency.

The next installment in this series will provide the design calculations to determine the minimum requirements for supply voltage, current drive capability and resultant power consumption and dissipation. In addition, heat management issues will be discussed. 